

# Micromachined Microwave Planar Spiral Inductors and Transformers

Renato P. Ribas, Jérôme Lescot, Jean-Louis Leclercq, Jean Michel Karam, *Member, IEEE*, and Fabien Ndagijimana

**Abstract**—A new micromachined planar spiral inductor, with the strips suspended individually, has been fabricated in standard GaAs high electron-mobility transistor monolithic-microwave integrated-circuit technology through maskless front-side bulk micromachining. The electronic compatibility, the use of industrial integrated-circuit production lines, the straightforward and low-cost additional procedure for structure releasing, and the very short etching time required to do such are the principal features related to such a novel inductor structure. Moreover, the air-gap layer created underneath the device and between the strips significantly reduces shunt and fringing parasitic capacitances, consequently increasing the performance and operating frequency range. Experimental measurements, carried out up to 15 GHz, before and after micromachining, showed for a 12-nH inductor an increase of the maximum  $Q$  factor from 5 (at 3 GHz) to about 20 (at 7 GHz), while the self-resonant frequency was shifted from 5 to 13 GHz. Furthermore, a structure with two interleaved spiral inductors, in a 1:1 transformer-like configuration, was also fabricated, and its performance was verified as well in order to demonstrate the promising performance improvements provided by the proposed device. Finally, heating and mechanical characteristics associated with freestanding microstructures are briefly evaluated using finite-element method simulations.

**Index Terms**—Inductors, micromachined devices, micromachining, MMIC, planar transformers, suspended microstrip.

## I. INTRODUCTION

THE increasing interest in monolithic microwave integrated circuits (MMIC's) today is due to several emergent applications, such as mobile wireless communication, satellite reception [global positioning system (GPS) and digital broadcasting satellite (DBS)], millimeter-wave radiometers, and automotive systems. Small size and weight, elimination of wire bonding, low power consumption, volume manufacturability, reliability, and reproducibility are some of numerous advantages of MMIC's in respect to discrete and hybrid components.

Despite recent advances in microelectronics processes, with the increasing cutoff frequency of silicon-based transistors (at gigahertz band) and level of integration of most GaAs integrated-circuit (IC) processes, passive components, such as transmission lines, planar inductors, and transformers still suffer from low performance at high frequencies due to losses and parasitic effects [1].

Therefore, a great effort has been done in order to improve the performance of such components, in particular, using the low-cost and mature silicon technology, by considering, e.g., multilevel interconnect processes, higher substrate resistivity, Cu metallization instead of Al, and freestanding devices [2]–[11]. Micromachining techniques, which are widely used to build monolithic integrated sensors and actuators [12], have also been proven very useful to enhance microwave passive devices through the construction of membrane-supported and shielded planar lumped elements [7]–[11]. However, specific processes or additional masking steps are usually required, and the electronic integration is somewhat compromised. The front-side bulk micromachining, on the other hand, seems to be the most efficient way to microelectromechanical system (MEMS) design, in terms of fabrication cost and electronic compatibility, since a straightforward maskless post-process etching is enough to release the structures [9]–[11].

This micromachining approach has been successfully used in a standard GaAs high electron-mobility transistor (HEMT) technology from Philips Microwave Limeil (PML), Limeil, France, and presents as the principal features the very small “open areas” (stack of dielectric and passivation openings needed to etch away the substrate material), the numerous suitable etchants without selective and preferential etching constraints, the compatibility to MMIC design, and all characteristics related to the GaAs material, i.e., high-temperature operation, piezoelectric effect, high thermal resistivity, high Seebeck coefficient, and so on [13].

In this paper, micromachined planar spiral inductors and transformers are presented. The open-area dimensions used herein for micromachining purposes allowed the construction of these devices with each spiral segment suspended individually. Such a novel structure is easier to fabricate than the well-known membrane-supported version because of the short etching time required. Furthermore, besides shunt capacitances, fringing parasitic effects, very critical in planar spiral transformers [14], [15], are also significantly reduced. The respective lumped equivalent models, analytical formulations, experimental measurements, heating, and mechanical characteristics are discussed in following sections.

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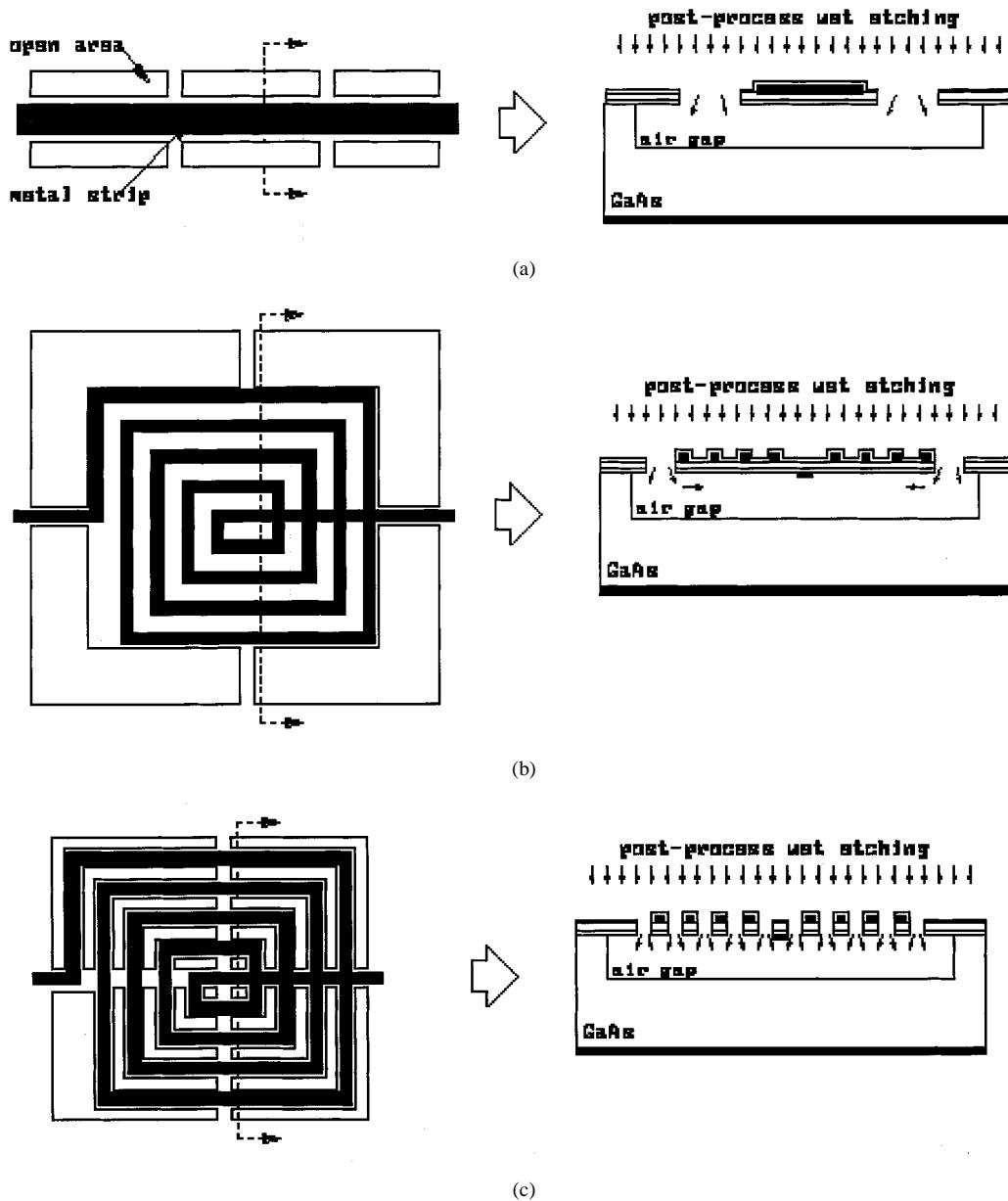


Fig. 1. Front-side bulk micromachined structures. (a) Suspended microstrip line. (b) Membrane-supported inductor. (c) Planar spiral inductor with strips suspended individually.

## II. MICROMACHINING DESCRIPTION

The front-side bulk micromachining approach relies on a post-process wet etching, with no modification in the standard IC fabrication, no additional masking, and no influence on the unconcerned electronic parts. Uncovered substrate surface regions (open areas), necessary to etch away portions of the bulk material, are created by stacking dielectric and passivation openings. As a result, bridges, cantilevers, membranes, and other geometries are easily constructed through the appropriate placement of open areas in the layout. The target technology is the  $0.2\text{-}\mu\text{m}$  GaAs HEMT D02AH process from PML, which provides a  $100\text{-}\mu\text{m}$ -thick GaAs substrate with backside ground plane for microstrip design [16]. The layout top view and cross section of a freestanding line is shown in Fig. 1(a). Note that

the minimum open area width allowed with this process is equal to  $4\text{ }\mu\text{m}$ .

Two types of suspended planar spiral inductors are possible using this approach: the membrane-supported version [see Fig. 1(b)], as presented by Chang *et al.* [9] in standard CMOS, and a novel structure with the strips suspended individually, taking advantage of the small open-area dimensions. As illustrated in Fig. 1(c), the etching time needed for complete suspension of such new version depends only on the linewidth and not on the total structure size or number of spiral turns. Large membranes, otherwise generally demand special attention in the etching procedures to avoid possible damages in the pad metallization and passivation layers caused by excessive etchant time exposure. Moreover, the elimination of the dielectric layers between the spiral wires contributes even more to

reduce the fringing capacitances. However, the heat dissipation represents an important drawback, as discussed in Section V.

After IC fabrication, a pre-cleaning step is applied on dies in order to remove eventual residual layers normally responsible for irregularities in the micromachine etching task. It is realized by dipping them in  $\text{HCl} : \text{H}_2\text{O}$  (1 : 10) – 20 s, then rinsing in deionized water – 10 s, dipping in  $\text{NH}_4\text{OH} : \text{H}_2\text{O}$  (1 : 1) – 20 s, and, finally, drying with nitrogen. The dies are then dipped in the etching solution, according to the specific parameters of concentration, temperature, and stirring. Selective and preferential etching characteristics are not taken into account since no GaAs material is kept underneath the structure. Therefore, a great number of GaAs etchants, such as  $\text{C}_6\text{H}_8\text{O}_7 : \text{H}_2\text{O}_2$  (citric acid)-,  $\text{H}_3\text{PO}_4$ -,  $\text{H}_2\text{SO}_4$ -, and  $\text{NH}_4\text{OH}$ -based solutions are suitable [17].

### III. THEORETICAL ANALYSIS AND LUMPED MODELS

#### A. Freestanding Microstrip

The equivalent lumped model of a microstrip transmission line, which represents a small subsection per unit length, is shown in Fig. 2(a). The circuit parameters  $R$ ,  $L$ ,  $C$ , and  $G$  are deduced at each frequency point from the propagation constant and characteristic impedance by using the classical Telegrapher's transmission —line equation [18]. The conductance  $G$  is usually neglected when a semiinsulating GaAs substrate is used. The series resistance  $R$ , on the other hand, is governed by the skin effect and can be computed using Pettenpaul's equation [19]

$$R = \frac{l}{wt\sigma} \left[ \frac{0.431x_w}{1 + 0.041(w/t)^{1.19}} + \frac{1.1147 + 1.2868x_w}{1.2296 + 1.287x_w^3} + 0.0035 \left( \frac{w}{t} - 1 \right)^{1.8} \right] \quad (1a)$$

for  $x_w \geq 2.5$  and

$$R = \frac{l}{wt\sigma} \left[ 1 + 0.0122x_w^{(3+0.01x_w^2)} \right] \quad (1b)$$

for  $x_w < 2.5$  and with  $x_w = (2\sigma\mu wt)^{1/2}$  a normalized frequency, where  $\sigma$  represents the conductivity,  $\mu$  is the permeability,  $w$  is the width, and  $t$  is the thickness of the metallic conductor with rectangular cross section.

Inductance  $L$ , per unit length, can be estimated by using the Grover formulation [20] and taking into account the ground-plane effects since the substrate thickness ( $h$ ) is low when compared to the microstrip length ( $l$ ) [21]

$$L = \frac{\mu_0 l}{2\pi} \left[ \ln \left( \frac{2h}{w+t} \right) + \frac{w+t}{3l} - \frac{2h}{l} + 1.5 \right]. \quad (2)$$

In fact, the capacitance  $C$  represents the most important parameter in this paper because it is directly affected by micromachining. A computer program based on a two-dimensional method of moments (MOM) has been used to evaluate the effective permittivity ( $\epsilon_{\text{eff}}$ ) of the microstrip line as a function of the air layer thickness. This analysis showed that it is not necessary to obtain high air-gap height because the  $\epsilon_{\text{eff}}$  decreases exponentially with the etching depth, as shown in Fig. 3. As a result, the capacitance between the wires and the backside ground

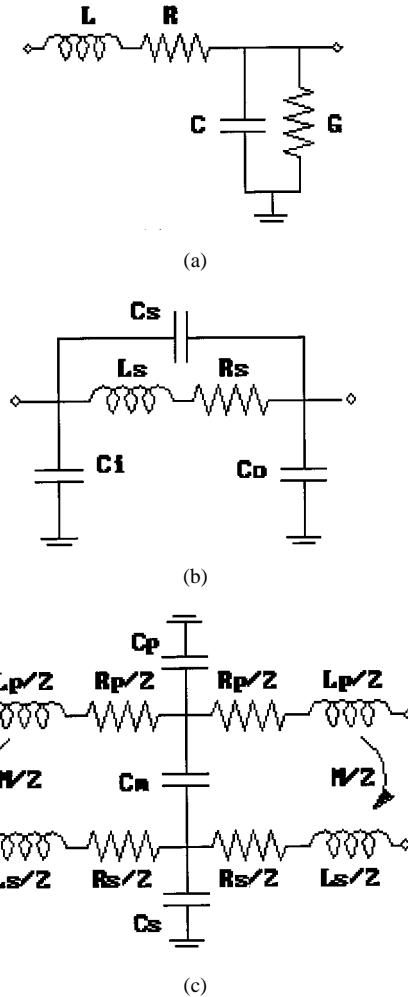


Fig. 2. Lumped-element equivalent models. (a) Microstrip line. (b) Planar inductor. (c) Transformer.

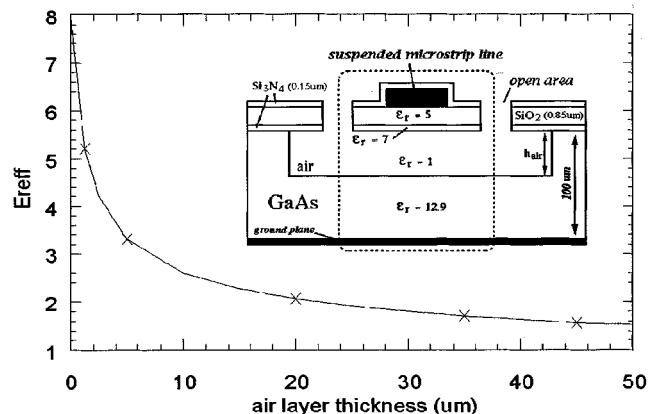


Fig. 3. Effective permittivity versus air-gap height of a suspended microstrip line.

plane is expected to reduce, e.g., twice by removing just 5% of the bulk material underneath the metal line.

#### B. Planar Spiral Inductor

The planar spiral inductor structure is known to be more compact and space efficient than the equivalent straight wire con-

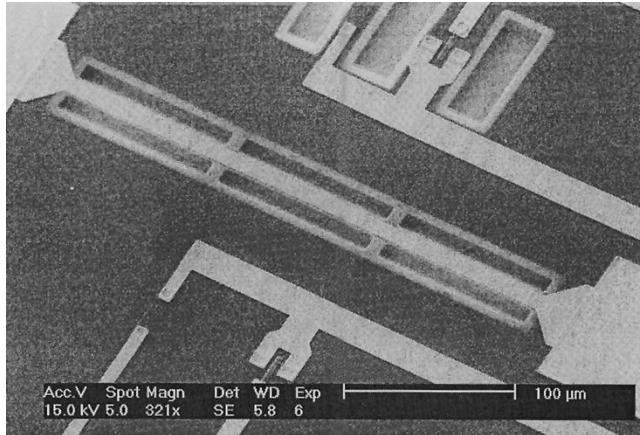


Fig. 4. Microphotograph of 0.5-mm-long suspended microstrip line.

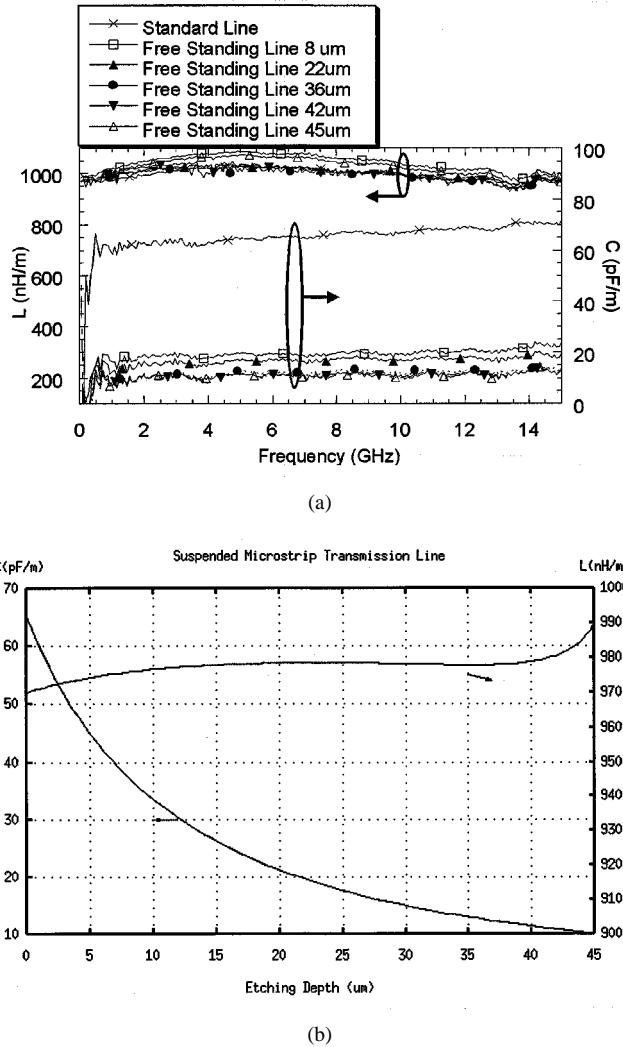


Fig. 5. Inductance and capacitance, per unit length, of 5  $\mu$ m-wide and 2 mm-long microstrip versus (a) frequency and (b) air-gap height-etching depth.

ductor. In the corresponding lumped-element equivalent circuit, illustrated in Fig. 2(b), the series branch is formed by the spiral

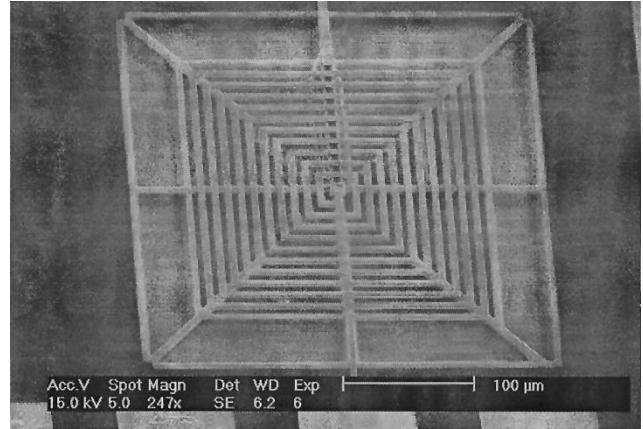


Fig. 6. Microphotograph of 12-nH planar spiral inductor with isolated strips.

inductance  $L_s$ , fringing capacitance  $C_s$ , and wire series resistance  $R_s$ . At first,  $L_s$  can be estimated using the equations proposed by Greenhouse [22]

$$L_s = \sum_{i=1}^N L_i + \sum_{i=1}^N \sum_{j=1}^N M_{ij} \quad (3)$$

where  $L_i$  represents the self-inductance of each straight segment  $i$ , and  $M_{ij}$  is the mutual inductance between the parallel segments  $i$  and  $j$ . The  $M_{ij}$  value is a function of the strips length ( $l$ ) and the distance between the track centers ( $d$ ), and can be calculated through the following equation:

$$M_{ij} = \frac{\mu_0 l}{2\pi} \left\{ \ln \left[ \frac{l}{D} + \sqrt{1 + \left( \frac{l}{D} \right)^2} \right] - \sqrt{1 + \left( \frac{D}{l} \right)^2} + \frac{D}{l} \right\} \quad (4)$$

where

$$\ln(D) = \ln(d) - \left[ \frac{1}{12} \left( \frac{w}{d} \right)^2 + \frac{1}{60} \left( \frac{w}{d} \right)^4 + \frac{1}{168} \left( \frac{w}{d} \right)^6 + \dots \right]. \quad (5)$$

Notice that  $M_{ij}$  is positive when the currents in two parallel conductors are in the same direction, and negative when they are in the opposite directions. This approach assumes that perpendicular segments present negligible mutual inductances. A more general form of (4) can be derived to calculate the mutual inductance of filamentary conductors with arbitrary lengths and without coincident ends [20]. Moreover, in order to consider the backside ground plane, an additional procedure includes the mutual inductance caused by a fictional mirror image, which is located at a distance of twice the substrate thickness from the actual spiral. The reduction in inductance value, in this case, is accounted for by the reverse current flow in the image spiral.

On the other hand,  $R_s$  is derived from (1a) and (1b) by considering the total length of the spiral inductor, while the series capacitance  $C_s$  accounts for the fringing capacitance between the spiral wires and between these wires and the center-tap underpass. The parasitics in the shunt branches are modeled by  $C_i$

TABLE I  
CHARACTERISTICS OF STANDARD AND MICROMACHINED PLANAR INDUCTOR WITH ISOLATED STRIPS

Air gap height (etching depth)	$R_s$ ( $\Omega$ )	$L_s$ (nH)	$C_o$ (fF)	$C_i$ (fF)	$C_s$ (fF)	$f_{res}$ (GHz)	$f_{Qmax}$ (GHz)	$Q_{max}$
standard	10.5	4.8	50	42	6	10.5	6.1	11.5
10 $\mu$ m	10.5	4.8	30	25	5	13.3	7.7	14.6
40 $\mu$ m	10.5	4.8	12	10	6	17.1	9.9	18.9
standard	30	12	65	50	10	5.3	3.1	5.1
8 $\mu$ m	28	12	50	45	6	6.2	3.6	6.3
22 $\mu$ m	29	12	31	29	6	7.6	4.4	7.5
42 $\mu$ m	29	12	6	3	6	13.4	7.7	13.3

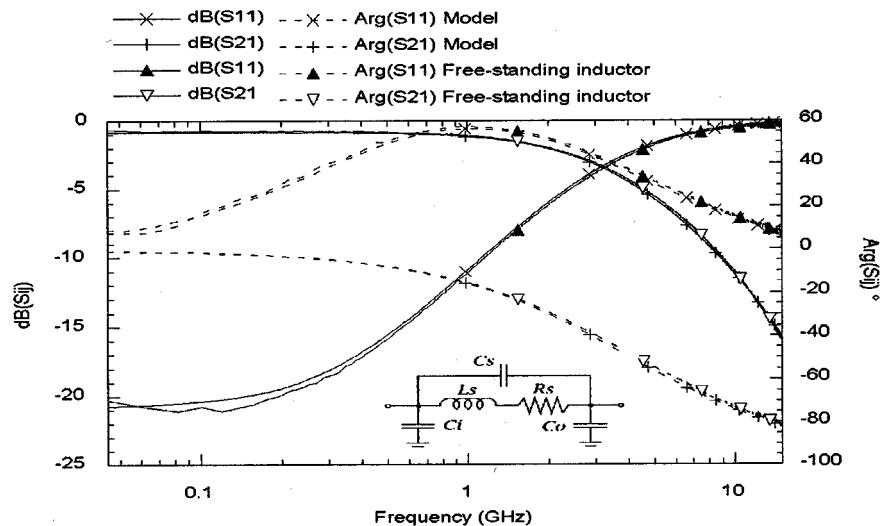


Fig. 7.  $S$ -parameter measurements versus inductor lumped model.

and  $C_o$ , which represent the substrate capacitances between the strips and ground plane, and can be computed with the two-dimensional (2-D) MOM technique, mentioned above, by considering a multiconductor structure.

The  $Q$  factor of the planar inductor, defined as the ratio of the imaginary part to the real part of the one-port input impedance with the other side grounded, can be calculated by using the following expression:

$$Q = \frac{\omega L_s}{R_s} \left[ 1 - \frac{R_s^2(C_s + C_o)}{L_s} - \omega^2 L_s(C_s + C_o) \right] \quad (6)$$

where the term in brackets represents the self-resonant factor which describes the reduction of the  $Q$  factor caused by parasitic capacitance effects. To illustrate the predicted improvements resulted from micromachining, a 15-nH inductor with 10- $\mu$ m-wide and 5- $\mu$ m-spacing segments was taken as a case of study, using the model element values provided by PML, i.e.,  $R_s = 23.4$ ,  $C_s = 2.2$  fF, and  $C_i = 200$  fF. Considering that  $C_i$  and  $C_s$  reduce three times, the maximum  $Q$  factor is expected to increase from 4.5 (at 1.6 GHz) to around 7.8 (at 2.9 GHz), and the resonant frequency may be shifted from 2.8 to 5.1 GHz.

### C. Planar Spiral Transformer

The spiral transformer structure, investigated herein, consists of two identical spiral inductors interwound. The lumped-element model proposed by Frlan *et al.* [14], and illustrated in Fig. 2(c), was adopted herein.  $R_1$  and  $R_2$  are the series resistance, while  $L_1$  and  $L_2$  are the total inductances of the primary and secondary, respectively, and, since the structure is formed by identical spiral inductors, these values are identical.  $M$  represents the mutual inductance between the coils.

Once again, the static self-inductance and mutual inductance between parallel segments are calculated according to the method described for planar inductors, always considering the ground-plane effects as well as the estimation of the segment-to-ground and the mutual interline capacitances. The capacitance between nonadjacent lines are neglected with no significant change in the final accuracy of the model, unlike the total inductance in which all the individual self-inductances must be accounted for.

## IV. RESULTS AND DISCUSSION

Prototypes containing test structures were fabricated using the commercial PML D02AH process through the circuit mul-

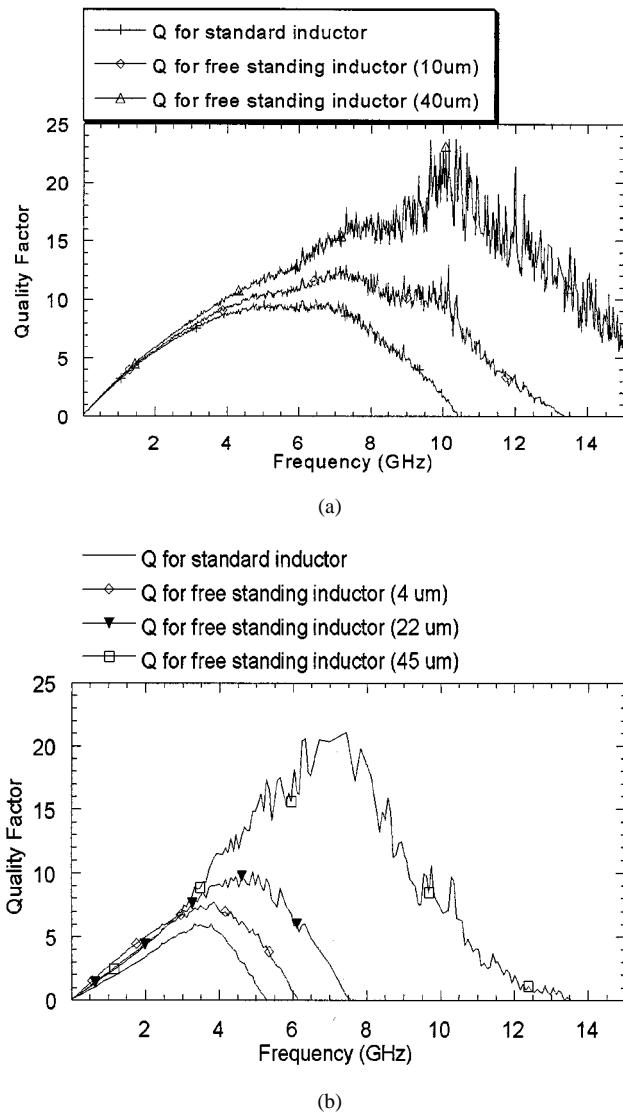


Fig. 8.  $Q$  factor versus air-gap height of (a) 4.9- and (b) 12-nH inductors.

tiproject (CMP) wafer service [23]. The dies were then exposed one by one to the post-fabrication wet etching, considering a wide range of etching time in order to obtain freestanding structures with different air-gap heights. Two-port  $S$ -parameter measurements were performed for the frequency range from 0.5 to 15 GHz, using the HP8510B network analyzer and a Cascade Microtech probe station. Open, short, thru, and 50 structures were available on a standard substrate for short open load thru (SOLT) calibration. Moreover, open-circuit test patterns were probed to measure pad parasitics for deembedding. The measured data were transmitted to a computer for automatic parameter extraction. Prior to each acquisition, an additional procedure based on the  $Y$ -parameter subtraction method was used to remove the parasitic effects from the probe pads [24].

#### A. Freestanding Microstrip

Suspended microstrip lines were constructed to evaluate the influence of micromachining in the  $L$  and  $C$  lumped model parameters (see Fig. 4). Dielectric arms, with 5- $\mu\text{m}$  width and 10- $\mu\text{m}$  length, were placed at each 100  $\mu\text{m}$  along the long lines

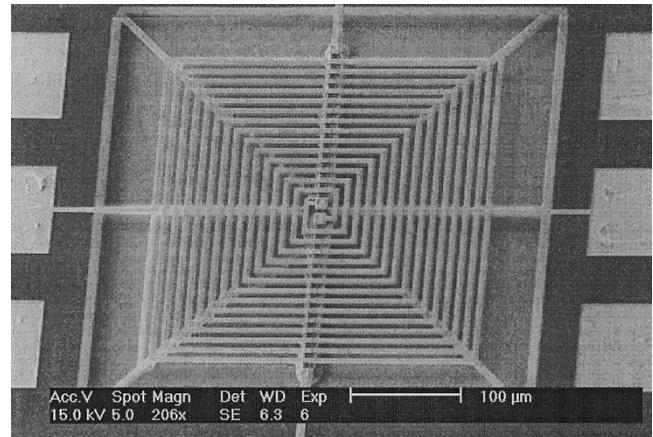


Fig. 9. Microphotograph of micromachined planar spiral transformer.

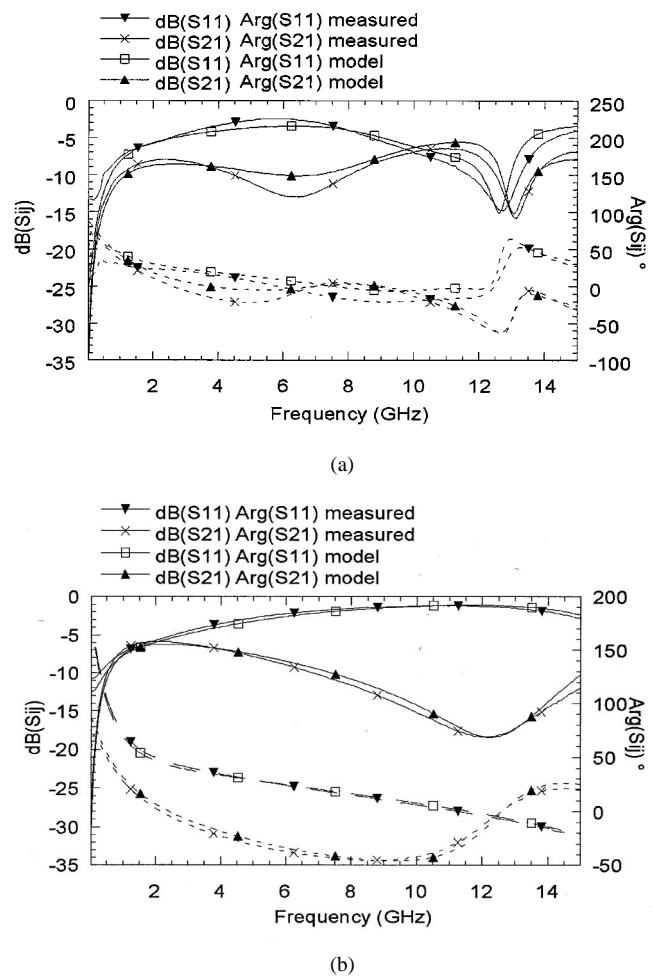


Fig. 10.  $S$ -parameter measurements versus lumped-element model of: (a) standard and (b) 42- $\mu\text{m}$ -depth suspended planar spiral transformer.

for mechanical support. Measurements have shown that both  $L$  and  $C$  are relatively frequency independent, as illustrated in Fig. 5(a). Moreover, in respect to the etching depth,  $C$  exhibited an exponential decreasing with the air layer thickness, agreeing as well with the computed effective permittivity discussed above [see Fig. 5(b)]. On the other hand,  $L$  is not really affected by micromachining because it is predominantly determined by the magnetic flux external to the conductor.

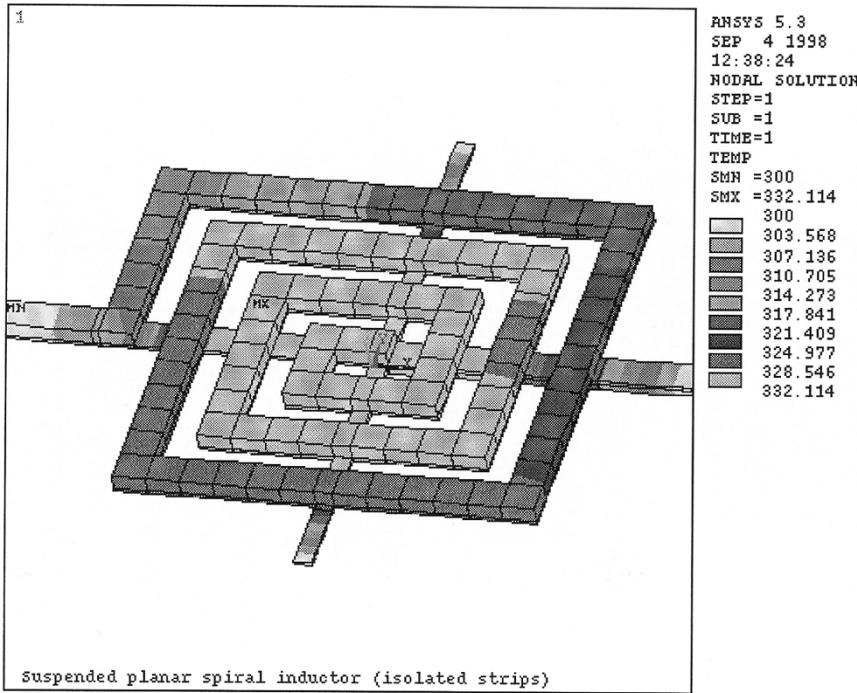


Fig. 11. FEM solid model: temperature distribution on micromachined planar inductors with isolated strips.

### B. Planar Spiral Inductor

Two planar spiral inductors were fabricated and post-process etched: a 4.9- and a 12-nH inductors composed by five and seven turns, respectively. Both inductors are formed by 5- $\mu\text{m}$ -wide and 5- $\mu\text{m}$ -spacing segments. In the case of the 12-nH inductor structure, the three most external spiral turns are supported by thin dielectric arms at four corners to prevent eventual mechanical fracture, as shown in Fig. 6.

The measured inductance, obtained from  $Y$ -parameters  $L_s = \text{Im}(1/y_{12})/\omega$  agrees well with the predicted theoretical values at low frequencies. Notice that the negative mutual inductance due to image spiral equal to 0.3 and 3.7 nH for the 4.9- and 12-nH inductors, respectively, was verified to be an important parameter in the lumped-element modeling. Moreover, the measured resistive component  $R_s = \text{Re}(1/y_{12})$  is closed to the dc resistance of the spiral line.

On the other hand, the extracted capacitances were obtained directly from  $C_i = \text{Im}(y_{11} + y_{12})/\omega$  and  $C_o = \text{Im}(y_{22} + y_{21})/\omega$ , and are summarized in Table I. As expected, a significant reduction was verified with the suspended structures. However, the  $C_s$  value was found to be predominantly determined by the spiral and center-tap underpass capacitance, not influenced by micromachining. As a result, the decreasing of fringing capacitances becomes more evident by increasing the number of spiral turns, as occurred in the 12-nH inductor.

The equivalent-element model behavior agrees well with the measured  $S$ -parameters, as illustrated in Fig. 7. As shown in Fig. 8, the  $Q$  factor, the frequency at the maximum  $Q$ , and the resonant frequency were significantly improved by micromachining. These characteristics are listed in Table I and were ob-

tained considering the average values of the element model parameters, also presented in this table.

### C. Planar Spiral Transformer

The fabricated micromachined transformer is composed by two interleaved seven-turn spiral inductors, presenting 6- $\mu\text{m}$ -wide and 6- $\mu\text{m}$ -spacing segments, as shown in Fig. 9. The extracted element values are  $L_p = L_s = 8.6$  nH,  $M = 6.8$  nH, and  $R_p = R_s = 30$ . Since the lowering in self inductance due to its own image spiral is 0.85 nH and the mutual inductance between one actual spiral and the image of the other is 0.8 nH, it is imperative to take into account the ground-plane effects on self and mutual inductances for the lumped model accuracy. The extracted capacitances were obtained equal to  $C_p = C_s = 40$  fF and  $C_m = 200$  fF for the standard transformer, they reduced to  $C_p = C_s = 15$  fF and  $C_m = 80$  fF in the micromachined structure, with an air-gap underneath the strips equals to 42  $\mu\text{m}$ . The comparison between measured and simulated  $S$ -parameters of standard and suspended transformers is shown in Fig. 10.

## V. HEATING AND MECHANICAL CHARACTERISTICS

Besides electrical performance, thermal and mechanical characteristics are also very important to verify the usefulness of these micromachined devices. It is well known that freestanding structures have been widely used in thermo-electrical-based micromachined devices, such as bolometers and thermopiles, since suspended parts present poor heat dissipation acting as “hot regions” either for temperature sensing

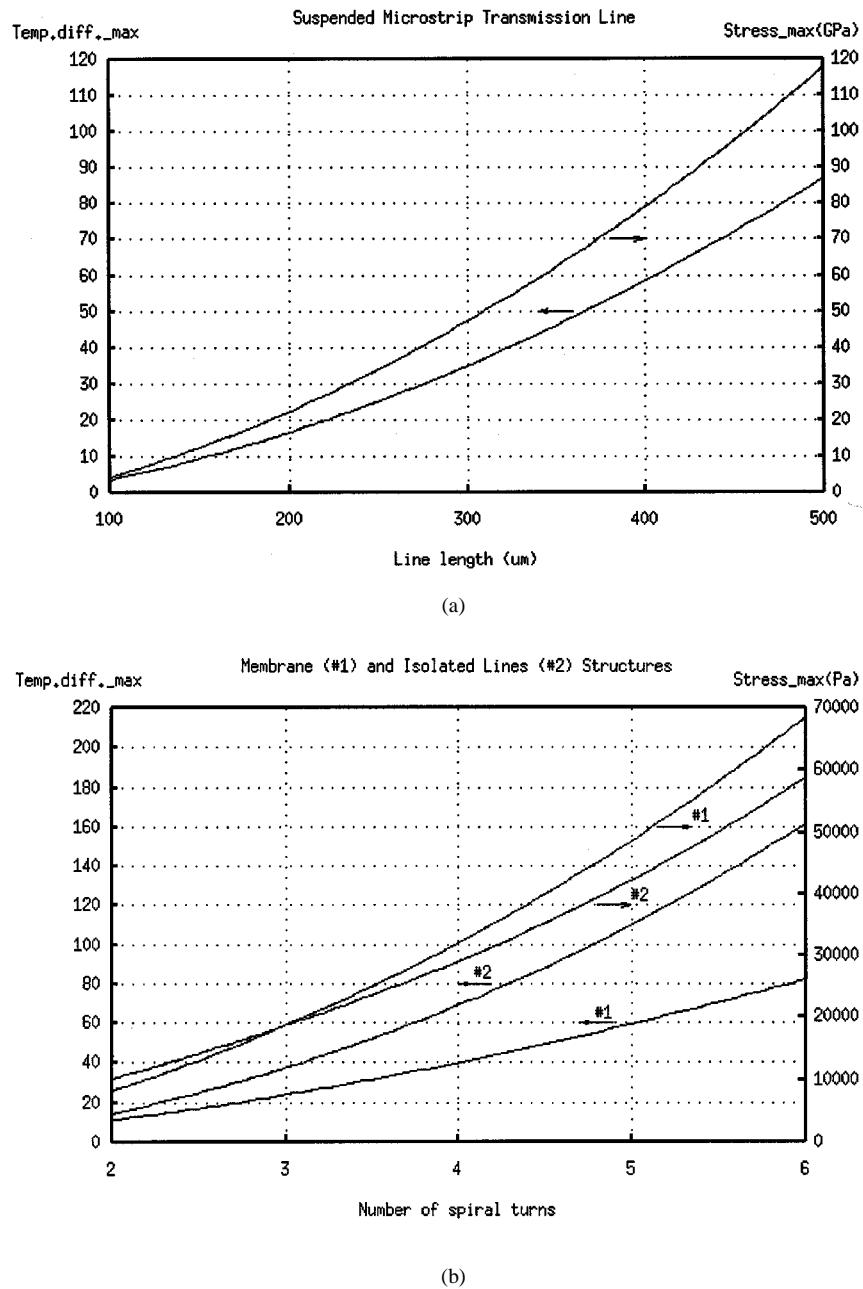


Fig. 12. Maximum temperature difference and mechanical stress of micromachined structures. (a) Microstrip line. (b) Planar spiral inductors over membrane and with isolated lines.

or to Seebeck voltage generation, considering the substrate as heat sink (“cold region”). However, in the case of suspended microwave passive devices, it represents a constraint due to the increasing series resistance of the wires. On the other hand, the mechanical constraints are essential to prove the structure applicability. A complete analysis of such characteristics was carried out through extensive finite-element method (FEM) simulations, as illustrated in Fig. 11.

#### A. Heat Distribution

The maximum temperature difference of a single and straight suspended microstrip line as a function of the

bridge length was obtained from FEM simulations using the worst-case current value, i.e., the maximum current determined by PML for the interconnection metal [see Fig. 12(a)]. Such behavior was observed almost invariant in terms of the linewidth. Moreover, both versions of planar spiral inductors, over a membrane and with isolated strips, were also investigated for the maximum current allowed. The maximum increasing temperature as a function of the number of spiral turns is shown in Fig. 12(b). Note that the heat dissipation is slightly better for the membrane structure. Furthermore, since the typical value of the temperature coefficient of resistivity (TCR) for metals is

usually  $5 \times 10^{-3}$  K, an increasing of  $100^\circ$  may result in 50% increasing of line series resistance, which directly influence the inductor  $Q$  factor.

### B. Mechanical Stress

In the mechanical evaluation, an acceleration of 100 g (i.e.,  $980 \text{ m/s}^2$ ) was used in FEM simulations. To have an idea about such acceleration value, air-bag accelerometers for automotive systems work at range of  $\pm 50$  g [25]. Similarly to temperature behavior, the maximum stress as well as the maximum displacement were also observed approximately invariant in respect to the microstrip width. In the case of suspended planar inductors, the maximum stress was obviously observed in the most external dielectric arms, and it is shown in Fig. 12(b) as a function of the number of spiral turns. Note that  $\text{SiO}_2$  presents the lowest fracture strength (50–55 MPa) among the structure layers. In other words, according to simulation results, this suspended inductor can be considered mechanically very robust. Nevertheless, it is suggested to use dielectric arms at four corners for larger spiral structures. Finally, the internal stress between the IC layers could be very critical, but it cannot be evaluated through such a type of simulation. A more detailed study about mechanical properties of micromachined devices is out of the scope of this paper.

## VI. CONCLUSIONS

The front-side bulk micromachining compatible to a standard GaAs HEMT technology has been demonstrated to be very useful for performance improvement of microwave passive devices, in particular, inductors and transformers. Such straightforward and cost-effective micromachining technique allowed the creation of a new and promising planar spiral inductor structure with the strips suspended separately, significantly reducing shunt and fringing capacitances. The self-resonant frequency and maximum  $Q$  factor of micromachined compounds have increased up to 250%. Moreover, mechanical constraints were verified as being not so critical, while careful attention must paid to heat dissipation depending on the electrical current used. Furthermore, the fact that the D02AH process from PML, considered in this paper, is available to MMIC design, filters, matching networks, and low-noise amplifiers, and other RF circuits can be directly enhanced by using such approach.

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